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## ZXLD1370

## 60V HIGH ACCURACY BUCK/BOOST/BUCK-BOOST LED DRIVER-CONTROLLER WITH AEC-Q100

## Description

The ZXLD1370 is an LED driver controller IC for driving external MOSFETs to drive high current LEDs. It is a multi-topology controller enabling it to efficiently control the current through series connected LEDs. The multi-topology enables it to operate in buck, boost and buck-boost configurations.

The 60 V capability coupled with its multi-topology capability enables it to be used in a wide range of applications and drive in excess of 15 LEDs in series.

The ZXLD1370 is a modified hysteretic controller using a patent pending control scheme providing high output current accuracy in all three modes of operation. High accuracy dimming is achieved through DC control and high frequency PWM control.

The ZXLD1370 uses two pins for fault diagnosis. A flag output highlights a fault, while the multi-level status pin gives further information on the exact fault.

## Features

- 0.5\% Typical Output Current Accuracy
- 6 V to 60 V Operating Voltage Range
- LED Driver Supports Buck, Boost and Buck-Boost Configurations
- Wide Dynamic Range Dimming
- 20:1 DC Dimming
- 1000:1 Dimming Range at 500 Hz
- Up to 1 MHz Switching
- High Temperature Control of LED Current Using TADJ
- Available in Automotive Grade with AEC-Q100 and TS16949 Certification
- Available in "Green" Molding Compound (No Br, Sb) with Lead Free Finish/ RoHS Compliant
- Totally Lead-Free \& Fully RoHS Compliant (Notes 1 \& 2)
- Halogen and Antimony Free. "Green" Device (Note 3)


## Pin Assignments



[^0]2. See http://www.diodes.com for more information about Diodes Incorporated's definitions of Halogen- and Antimony-free, "Green" and Lead-free.
3. Halogen- and Antimony-free "Green" products are defined as those which contain $<900 \mathrm{ppm}$ bromine, $<900 \mathrm{ppm}$ chlorine ( $<1500 \mathrm{ppm}$ total $\mathrm{Br}+\mathrm{Cl}$ ) and <1000ppm antimony compounds.

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## Typical Applications Circuit



Buck-Boost Diagram Utilizing Thermistor and TADJ


## Functional Block Diagram



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## Pin Descriptions

| Pin Name | Pin | Type (Note 4) | Function |
| :---: | :---: | :---: | :---: |
| ADJ | 1 | 1 | Adjust input (for dc output current control). <br> Connect to REF to set $100 \%$ output current. <br> Drive with dc voltage ( $125 \mathrm{mV}<\mathrm{V}_{\mathrm{ADJ}}<2.5 \mathrm{~V}$ ) to adjust output current from $10 \%$ to $200 \%$ of set value. The ADJ pin has an internal clamp that limits the internal node to less than 3 V . This provides some failsafe should they get overdriven. |
| REF | 2 | 0 | Internal 1.25V reference voltage output. |
| TADJ | 3 | 1 | Temperature Adjust input for LED thermal current control. <br> Connect thermistor/resistor network to this pin to reduce output current above a preset temperature threshold. <br> Connect to REF to disable thermal compensation function. (See section on thermal control.) |
| SHP | 4 | I/O | Shaping capacitor for feedback control loop. <br> Connect $100 \mathrm{pF} \pm 20 \%$ capacitor from this pin to ground to provide loop compensation. |
| STATUS | 5 | 0 | Operation status output (analog output) <br> Pin is at 4.5 V (nominal) during normal operation. <br> Pin switches to a lower voltage to indicate specific operation warnings or fault conditions. (See section on STATUS output.) <br> Status pin voltage is low during shutdown mode. |
| SGND | 6 | P | Signal ground (Connect to 0V) |
| PGND | 7 | P | Power ground - Connect to 0 V and pin 8 to maximize copper area |
| N/C | 8 | - | Not Connected internally - recommend connection to pin 7, (PGND), to maximize PCB copper for thermal dissipation |
| N/C | 9 |  | Not Connected internally - recommend connection pin 10 (GATE) to permit wide copper trace to gate of MOSFET |
| GATE | 10 | 0 | Gate drive output to external NMOS transistor - connect to pin 9 |
| $V_{\text {Aux }}$ | 11 | P | Auxiliary positive supply to internal switch gate driver. <br> Connect to $\mathrm{V}_{\mathrm{IN}}$, or auxiliary supply from 6 V to 15 V supply to reduce internal power dissipation (Refer to application section for more details) <br> Decouple to ground with capacitor close to device (refer to Applications section) |
| $\mathrm{V}_{\text {IN }}$ | 12 | P | Input supply to device ( 6 V to 60 V ). <br> Decouple to ground with capacitor close to device (refer to Applications section) |
| ISM | 13 | I | Current monitor input. Connect current sense resistor between this pin and $\mathrm{V}_{\mathrm{IN}}$ The nominal voltage across the resistor is 225 mV |
| FLAG | 14 | 0 | Flag open drain output. <br> Pin is high impedance during normal operation <br> Pin switches low to indicate a fault, or warning condition |
| PWM | 15 | 1 | Digital PWM output current control. <br> Pin driven either by open Drain or push-pull 3.3 V or 5 V logic levels. <br> Drive with frequency higher than 100 Hz to gate output 'on' and 'off' during dimming control. <br> The device enters standby mode when PWM pin is driven with logic low level for more than 15 ms nominal (Refer to application section for more details) |
| GI | 16 | 1 | Gain setting input. <br> Used to set the device in Buck mode or Boost, Buck-boost modes <br> Connect to ADJ in Buck mode operation <br> For Boost and Buck-boost modes, connect to resistive divider from ADJ to SGND. This defines the ratio of switch current to LED current (see application section). The GI pin has an internal clamp that limits the internal node to less than 3 V . This provides some failsafe should they get overdriven |
| EP | PAD | P | Exposed paddle. Connect to 0 V plane for electrical and thermal management |

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| Absolute Maximum Ratings (Note 5) (Voltages to GND, unless otherwise specified.) |  |  |  |
| :---: | :---: | :---: | :---: |
| Symbol | Parameter | Rating | Unit |
| $\mathrm{V}_{\text {IN }}$ | Input Supply Voltage Relative to GND | -0.3 to +65 | V |
| $\mathrm{V}_{\text {AUX }}$ | Auxiliary Supply Voltage Relative to GND | -0.3 to +65 | V |
| VISM | Current Monitor Input Relative to GND | -0.3 to +65 | V |
| $V_{\text {SENSE }}$ | Current Monitor Sense Voltage ( $\mathrm{V}_{\text {IN }}-\mathrm{V}_{\text {ISM }}$ ) | -0.3 to +5 | V |
| $V_{\text {GATE }}$ | Gate Driver Output Voltage | -0.3 to +20 | V |
| $l_{\text {GATE }}$ | Gate Driver Continuous Output Current | 18 | mA |
| $V_{\text {FLAG }}$ | Flag Output Voltage | -0.3 to 40 | V |
| $\mathrm{V}_{\mathrm{Pwm}}, \mathrm{V}_{\mathrm{ADJ}}$, $\mathrm{V}_{\text {TADJ, }}, \mathrm{V}_{\mathrm{GI}}$ | Other Input Pins | -0.3 to +5.5 | V |
| TJ | Maximum Junction Temperature | 150 | ${ }^{\circ} \mathrm{C}$ |
| $\mathrm{T}_{\text {ST }}$ | Storage Temperature | -55 to +150 | ${ }^{\circ} \mathrm{C}$ |

Stresses greater than the 'Absolute Maximum Ratings' specified above, may cause permanent damage to the device. These are stress ratings only; functional operation of the device at these or any other conditions exceeding those indicated in this specification is not implied. Device reliability may be affected by exposure to absolute maximum rating conditions for extended periods of time.

Semiconductor devices are ESD sensitive and may be damaged by exposure to ESD events. Suitable ESD precautions should be taken when handling and transporting these devices.

## Package Thermal Data

| Thermal Resistance | Package | Typical | Unit |
| :--- | :---: | :---: | :---: |
| Junction-to-Ambient, $\theta_{\mathrm{JA}}$ (Note 6) | TSSOP-16EP | 50 | ${ }^{\circ} \mathrm{C} / \mathrm{W}$ |
| Junction-to-Case, $\theta_{\mathrm{JC}}$ | TSSOP-16EP | 23 | ${ }^{\circ} \mathrm{C} / \mathrm{W}$ |

$\begin{array}{ll}\text { Notes: } & \text { 5. For correct operation SGND and PGND should always be connected together. } \\ & \text { 6. Measured on High Effective Thermal Conductivity Test Board" according JESD51. }\end{array}$

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Recommended Operating Conditions $\left(@ T_{\mathrm{A}}=+25^{\circ} \mathrm{C}\right.$, unless otherwise specified.)

| Symbol | Parameter | Performance/Comment | Min | Max | Unit |
| :---: | :---: | :---: | :---: | :---: | :---: |
| V IN | Input supply voltage range | Normal operation | 8 | 60 | V |
|  |  | Reduced performance operation (Note 7) | 6.3 |  |  |
| $\mathrm{V}_{\text {AUX }}$ | Auxiliary supply voltage range (Note 8) | Normal operation | 8 | 60 | V |
|  |  | Reduced performance operation (Note 7) | 6.3 |  |  |
| VISM | Current sense monitor input range |  | 6.3 | 60 | V |
| $\mathrm{V}_{\text {SENSE }}$ | Differential input voltage | $\mathrm{V}_{\text {VIN }}-\mathrm{V}_{\text {ISM }}$, with $0 \leq \mathrm{V}_{\text {ADJ }} \leq 2.5$ | 0 | 450 | mV |
| $V_{\text {ADJ }}$ | External dc control voltage applied to ADJ pin to adjust output current | DC brightness control mode from 10\% to 200\% | 0.125 | 2.5 | V |
| $\mathrm{I}_{\text {REF }}$ | Reference external load current | REF sourcing current |  | 1 | mA |
| $\mathrm{f}_{\text {max }}$ | Recommended switching frequency range (Note 9) |  | 300 | 1000 | kHz |
| $\mathrm{V}_{\text {TADJ }}$ | Temperature adjustment ( $\mathrm{T}_{\text {ADJ }}$ ) input voltage range |  | 0 | $V_{\text {ReF }}$ | V |
| fpwm | Recommended PWM dimming frequency range | To achieve 1000:1 resolution | 100 | 500 | Hz |
|  |  | To achieve 500:1 resolution | 100 | 1000 | Hz |
| tPWMH/L | PWM pulse width in dimming mode | PWM input high or low | 0.002 | 10 | ms |
| $\mathrm{V}_{\text {PWM }}$ | PWM pin high level input voltage |  | 2 | 5.5 | V |
| $\mathrm{V}_{\text {PWML }}$ | PWM pin low level input voltage |  | 0 | 0.4 | V |
| $\mathrm{T}_{\mathrm{J}}$ | Operating Junction Temperature Range |  | -40 | 125 | ${ }^{\circ} \mathrm{C}$ |
| GI | Gain setting ratio for boost and buck-boost modes | Ratio $=\mathrm{V}_{\mathrm{G} /} / \mathrm{V}_{\text {ADJ }}$ | 0.20 | 0.50 |  |

Notes: 7. Device starts up above 6 V and as such the minimum applied supply voltage has to be above 6.5 V (plus any noise margin). The ZXLD1370 will, however, continue to function when the input voltage is reduced from $\geq 8 \mathrm{~V}$ down to 6.3 V . When operating with input voltages below 8 V the output current and device parameters may deviate from their normal values; and is dependent on power MOSFET switch, load and ambient temperature conditions. To ensure best operation in Boost and Buck-Boost modes with input voltages, $\mathrm{V}_{\mathrm{IN}}$, between 6.3 and 8 V a suitable boot-strap network on $\mathrm{V}_{\mathrm{AUX}}$ pin is recommended. Performance in Buck mode will be reduced at input voltages ( $\mathrm{V}_{\text {IN }}, \mathrm{V}_{\mathrm{AUX}}$ ) below 8 V . - a boot-strap network cannot be implemented in buck mode.
8. $\mathrm{V}_{\text {AUX }}$ can be driven from a voltage higher than $\mathrm{V}_{\text {IN }}$ to provide higher efficiency at low $\mathrm{V}_{\mathrm{IN}}$ voltages, but to avoid false operation; a voltage should not be applied to $\mathrm{V}_{\mathrm{Au}}$ in the absence of a voltage at $\mathrm{V}_{\mathrm{IN}}$.
9. The device contains circuitry to control the switching frequency to approximately 400 kHz . The maximum and minimum operating frequency is not tested in production.

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## Electrical Characteristics (Note 5 ) ( $\mathrm{V}_{\mathrm{IN}}=\mathrm{V}_{\mathrm{AUX}}=12 \mathrm{~V}, \mathrm{~T}_{\mathrm{A}}=+25^{\circ} \mathrm{C}$, unless otherwise specified.)

| Symbol | Parameter | Conditions | Min | Typ | Max | Units |
| :---: | :---: | :---: | :---: | :---: | :---: | :---: |
| Supply and Reference Parameters |  |  |  |  |  |  |
| Vuv- | Under-Voltage detection threshold Normal operation to switch disabled | $\mathrm{V}_{\text {IN }}$ or $\mathrm{V}_{\text {AUx }}$ falling | 5.2 | 5.6 | 6.3 | V |
| Vuv+ | Under-Voltage detection threshold Switch disabled to normal operation | $\mathrm{V}_{\text {IN }}$ or $\mathrm{V}_{\text {AUX }}$ rising | 5.5 | 6.0 | 6.5 | V |
| $\mathrm{I}_{\mathrm{Q} \text {-IN }}$ | Quiescent current into $\mathrm{V}_{\text {IN }}$ | PWM pin floating. Output not switching |  | 1.5 | 3.0 | mA |
| $\mathrm{I}_{\mathrm{Q}-\mathrm{AUX}}$ | Quiescent current into $V_{\text {AUX }}$ |  |  | 150 | 300 | $\mu \mathrm{A}$ |
| $\mathrm{I}_{\text {SB-IN }}$ | Standby current into $\mathrm{V}_{\text {IN }}$. | PWM pin grounded for more than 15 ms |  | 90 | 150 | $\mu \mathrm{A}$ |
| ISB-AUX | Standby current into V ${ }_{\text {AUX }}$. |  |  | 0.7 | 10.0 | $\mu \mathrm{A}$ |
| $\mathrm{V}_{\text {REF }}$ | Internal reference voltage | No load | 1.237 | 1.250 | 1.263 | V |
| $\Delta \mathrm{V}_{\text {REF }}$ | Change in reference voltage with output current | Sourcing 1mA | -5 |  |  | mV |
|  |  | Sinking 100 $\mu \mathrm{A}$ |  |  | 5 |  |
| $\mathrm{V}_{\text {REF_LINE }}$ | Reference voltage line regulation | $\mathrm{V}_{\text {IN }}=\mathrm{V}_{\text {AUX }}, 6.5 \mathrm{~V}<\mathrm{V}_{\text {IN }}=<60 \mathrm{~V}$ | -60 | -90 |  | dB |
| $\mathrm{V}_{\text {Ref-ti }}$ | Reference temperature coefficient |  |  | +/-50 |  | ppm/ $/{ }^{\circ} \mathrm{C}$ |
| DC-DC Converter Parameters |  |  |  |  |  |  |
| $V_{\text {AdJ }}$ | External dc control voltage applied to ADJ pin to adjust output current (Note 8) | DC brightness control mode $10 \%$ to $200 \%$ | 0.125 | 1.25 | 2.50 | V |
| $I_{\text {ADJ }}$ | ADJ input current (Note 10) | $\begin{aligned} & \mathrm{V}_{\mathrm{ADJ}} \leq 2.5 \mathrm{~V} \\ & \mathrm{~V}_{\mathrm{ADJ}}=5.0 \mathrm{~V}^{\dagger} \end{aligned}$ |  |  | $\begin{gathered} 100 \\ 5 \end{gathered}$ | $\begin{aligned} & \mathrm{nA} \\ & \mu \mathrm{~A} \end{aligned}$ |
| $\mathrm{V}_{\mathrm{GI}}$ | GI Voltage threshold for boost and buck-boost modes selection (Note 8) | $\mathrm{V}_{\text {ADJ }}=1.25 \mathrm{~V}$ |  |  | 0.8 | V |
| IGI | GI input current (Note 10) | $\begin{aligned} & \mathrm{V}_{\mathrm{GI}} \leq 2.5 \mathrm{~V} \\ & \mathrm{~V}_{\mathrm{GI}}=5.0 \mathrm{~V}^{\dagger} \end{aligned}$ |  |  | $\begin{gathered} 100 \\ 5 \end{gathered}$ | $\begin{aligned} & \mathrm{nA} \\ & \mu \mathrm{~A} \end{aligned}$ |
| IPWM | PWM input current | $\mathrm{V}_{\text {PWM }}=5.5 \mathrm{~V}$ |  | 36 | 100 | $\mu \mathrm{A}$ |
| tpWMoff | PWM pulse width (to enter shutdown state) | PWM input low | 10 | 15 | 25 | ms |
| TsDH | Thermal shutdown upper threshold (GATE output forced low) | Temperature rising. |  | 150 |  | ${ }^{\circ} \mathrm{C}$ |
| TsdL | Thermal shutdown lower threshold (GATE output re-enabled) | Temperature falling. |  | 125 |  | ${ }^{\circ} \mathrm{C}$ |
| High-Side Current Monitor (Pin ISM) |  |  |  |  |  |  |
| ISM | Input Current | @ VISM $=12 \mathrm{~V}$ |  | 11 | 20 | $\mu \mathrm{A}$ |
| $\mathrm{V}_{\text {SENSE }}$ | Current measurement sinse voltage | Buck |  | 218 |  | mV |
|  |  | Boost (Note 11) $\mathrm{V}_{\text {ADJ }}=1.25 \mathrm{~V}$ |  | 225 |  |  |
|  |  | Buck-Boost (Note 11) |  |  |  |  |
| $V_{\text {SENSE_acc }}$ | Accuracy of nominal $\mathrm{V}_{\text {SENSE }}$ threshold voltage | $\mathrm{V}_{\mathrm{ADJ}}=1.25 \mathrm{~V}$ |  | $\pm 0.25$ | $\pm 2$ | \% |
| $\mathrm{V}_{\text {SENSE-OC }}$ | Over-current sense threshold voltage |  | 300 | 350 | 375 | mV |

Notes: 10. The ADJ and GI pins have an internal clamp that limits the internal node to less than 3 V . This provides some failsafe should those pins get overdriven. 11. Initial sense voltage in Boost and Buck-Boost modes at maximum duty cycle.

Electrical Characteristics (cont.) $\left(\mathrm{V}_{\mathbb{I N}}=\mathrm{V}_{\mathrm{AUX}}=12 \mathrm{~V}, \mathrm{~T}_{\mathrm{A}}=+25^{\circ} \mathrm{C}\right.$, unless otherwise specified.)

| Symbol | Parameter | Conditions | Min | Typ | Max | Units |
| :---: | :---: | :---: | :---: | :---: | :---: | :---: |
| Output Parameters |  |  |  |  |  |  |
| $\mathrm{V}_{\text {FLAGL }}$ | FLAG pin low level output voltage | Output sinking 1mA |  |  | 0.5 | V |
| Iflagoff | FLAG pin open-drain leakage current | $\mathrm{V}_{\text {FLAG }}=40 \mathrm{~V}$ |  |  | 1 | $\mu \mathrm{A}$ |
| V ${ }_{\text {status }}$ | STATUS Flag no-load output voltage (Note 12) | Normal operation | 4.2 | 4.5 | 4.8 | V |
|  |  | Out of regulation ( $\mathrm{V}_{\text {SHP }}$ out of range) (Note 13) | 3.3 | 3.6 | 3.9 |  |
|  |  | $\mathrm{V}_{\text {IN }}$ under-voltage ( $\mathrm{V}_{\text {IN }}<5.6 \mathrm{~V}$ ) | 3.3 | 3.6 | 3.9 |  |
|  |  | Switch stalled (ton or toff $>100 \mu \mathrm{~s}$ ) | 3.3 | 3.6 | 3.9 |  |
|  |  | Over-temperature ( $\mathrm{T}_{\mathrm{J}}>+125^{\circ} \mathrm{C}$ ) | 1.5 | 1.8 | 2.1 |  |
|  |  | Excess sense resistor current $\left(V_{\text {SENSE }}>0.32 \mathrm{~V}\right)$ | 0.6 | 0.9 | 1.2 |  |
| $\mathrm{R}_{\text {status }}$ | Output impedance of STATUS output | Normal operation |  | 10 |  | k $\Omega$ |
| Driver output (PIN GATE) |  |  |  |  |  |  |
| VGateh | High level output voltage | No load Sourcing 1mA (Note 14) | 10 | 11 |  | V |
| $V_{\text {GATEL }}$ | Low level output voltage | Sinking 1mA, (Note 15) |  |  | 0.5 | V |
| VGatecl | High level GATE CLAMP voltage | $\begin{aligned} & \mathrm{V}_{I N}=\mathrm{V}_{\mathrm{AU}} \mathrm{X}=\mathrm{V}_{\mathrm{ISM}}=18 \mathrm{~V} \\ & \mathrm{I}_{\text {GATE }}=1 \mathrm{~mA} \end{aligned}$ |  | 12.8 | 15.0 | V |
| IGATE | Dynamic peak current available during rise or fall of output voltage | Charging or discharging gate of external switch with $Q_{G}=10 \mathrm{nC}$ and 400 kHz |  | $\pm 300$ |  | mA |
| $\mathrm{tstall}^{\text {sta }}$ | Time to assert 'STALL' flag and warning on STATUS output (Note 16) | GATE low or high |  | 100 | 170 | $\mu \mathrm{s}$ |
| LED Thermal control circuit ( $\mathrm{T}_{\text {ADJ }}$ ) parameters |  |  |  |  |  |  |
| $\mathrm{V}_{\text {TADJH }}$ | Upper threshold voltage | Onset of output current reduction ( $\mathrm{V}_{\text {TADJ }}$ falling) | 560 | 625 | 690 | mV |
| $\mathrm{V}_{\text {TADJL }}$ | Lower threshold voltage | Output current reduced to < $10 \%$ of set value ( $\mathrm{V}_{\text {TADJ }}$ falling) | 380 | 440 | 500 | mV |
| Itadj | T ${ }_{\text {ADJ }}$ pin Input current | $\mathrm{V}_{\text {TADJ }}=1.25 \mathrm{~V}$ |  |  | 1 | $\mu \mathrm{A}$ |

Notes: 12. In the event of more than one fault/warning condition occurring, the higher priority condition will take precedence. E.g. 'Excessive coil current' and 'Out of regulation' occurring together will produce an output of 0.9 V on the STATUS pin. The voltage levels on the STATUS output assume the Internal regulator to be in regulation and $\mathrm{V}_{\mathrm{ADJ}}<=\mathrm{V}_{\text {REF }}$. A reduction of the voltage on the STATUS pin will occur when the voltage on $\mathrm{V}_{\text {IN }}$ is near the minimum value of 6 V .
13. Flag is asserted if $\mathrm{V}_{\mathrm{SHP}}<2.5 \mathrm{~V}$ or $\mathrm{V}_{\mathrm{SHP}}>3.5 \mathrm{~V}$
14. GATE is switched to the supply voltage $\mathrm{V}_{\text {AUx }}$ for low values of $\mathrm{V}_{\text {AUX }}$ (i.e. between 6 V and approximately 12 V ). For $\mathrm{V}_{\mathrm{AUX}}>12 \mathrm{~V}$, GATE is clamped internally to prevent it exceeding 15 V .
15. GATE is switched to PGND by an NMOS transistor
16. If $\mathrm{t}_{\mathrm{ON}}$ exceeds $\mathrm{t}_{\text {stall }}$, the device will force GATE low to turn off the external switch and then initiate a restart cycle. During this phase, ADJ is grounded internally and the SHP pin is switched to its nominal operating voltage, before operation is allowed to resume. Restart cycles will be repeated automatically until the operating conditions are such that normal operation can be sustained. If $t_{\text {OFF }}$ exceeds $t_{\text {StALL }}$, the switch will remain off until normal operation is possible.

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## Typical Characteristics



Figure 1 Supply Current vs. Supply Voltage


Figure 3 LED Current vs. $\mathrm{T}_{\text {ADJ }}$ Voltage


Figure $2 \mathrm{~V}_{\text {REF }}$ vs. Temperature


Figure $4 \mathrm{I}_{\text {Led }}$ vs. PWM Duty Cycle

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Typical Characteristics (cont.)


Figure 5 Buck LED Current, Switching Frequency vs. $\mathrm{V}_{\mathrm{ADJ}}$


Figure 7 Boost LED Current, Switching Frequency vs. $V_{\text {ADJ }}$


Figure 6 Buck-Boost LED Current, Switching Frequency vs. $\mathrm{V}_{\mathrm{ADJ}}$


Figure 8 Duty Cycle vs. Input Voltage

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Typical Characteristics (cont.) Buck Mode $-\mathrm{R}_{\mathrm{S}}=150 \mathrm{~m} \Omega, \mathrm{~L}=33 \mu \mathrm{H}$


Figure 9 Load Current vs. Input Voltage \& Number of LED


Figure 10 Frequency vs. Input Voltage \& Number of LED


Figure 11 Efficiency vs. Input \& Number of LED

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Typical Characteristics (cont.) Buck Mode $-\mathrm{R}_{\mathrm{S}}=300 \mathrm{~m} \Omega, \mathrm{~L}=47 \mathrm{\mu H}$


Figure $12 \mathrm{I}_{\text {LED }}$ vs. Input \& Number of LED


Figure 13 Frequency ZXLD1370-Buck Mode - L47 $\mu \mathrm{H}$


Figure 14 Efficiency vs. Input Voltage \& Number of LED

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Typical Characteristics (cont.) Boost Mode $-\mathrm{R}_{\mathrm{S}}=150 \mathrm{~m} \Omega, \mathrm{G}_{\text {RATIO }}=0.23, \mathrm{~L}=33 \mu \mathrm{H}$


Figure $15 \mathrm{I}_{\text {LED }}$ vs. Input Voltage \& Number of LED


Figure 16 Frequency vs. Input Voltage \& Number of LED


Figure 17 Efficiency vs. Input Voltage \& Number of LED

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Typical Characteristics (cont.) Buck-Boost Mode $-\mathrm{R}_{\mathrm{S}}=150 \mathrm{~m} \Omega, \mathrm{GI}_{\text {RATIO }}=0.23, \mathrm{~L}=47 \mathrm{H} \mathrm{H}$


Figure 18 LED Current vs. Input Voltage \& Number of LED


Figure 19 Switching Frequency vs. Input Voltage \& Number of LED


Figure 20 Efficiency vs. Input Voltage \& Number of LED

## Application Information

The ZXLD1370 is a high accuracy hysteretic inductive buck/boost/buck-boost controller designed to be used with an external NMOS switch for current-driving single or multiple series-connected LEDs. The device can be configured to operate in buck, boost, or buck-boost modes by suitable configuration of the external components as shown in the schematics shown in the device operation description.

## Device Description

## a) Buck mode - the most simple buck circuit is shown in Figure 21

 Control of the LED current buck mode is achieved by sensing the coil current in the sense resistor Rs, connected between the two inputs of a current monitor within the control loop block. An output from the control loop drives the input of a comparator which drives the gate of the external NMOS switch transistor Q1 via the internal Gate Driver. When the switch is on, the drain voltage of Q1 is near zero. Current flows from VIN, via Rs, LED, coil and switch to ground. This current ramps up until an upper threshold value is reached (see Figure 22). At this point GATE goes low, the switch is turned off and the drain voltage increases to VIN plus the forward voltage, VF, of the schottky diode D1. Current flows via RS, LED, coil and D1 back to VIN. When the coil current has ramped down to a lower threshold value, GATE goes high, the switch is turned on again and the cycle of events repeats, resulting in continuous oscillation. The feedback loop adjusts the NMOS switch duty cycle to stabilize the LED current in response to changes in external conditions, including input voltage and load voltage.The average current in the sense resistor, LED and coil is equal to the average of the maximum and minimum threshold currents. The ripple current (hysteresis) is equal to the difference between the thresholds. The control loop maintains the average LED current at the set level by adjusting the switch duty cycle continuously to force the average sense resistor current to the value demanded by the voltage on the ADJ pin. This minimizes variation in output current with changes in operating conditions.

The control loop also regulates the switching frequency by varying the level of hysteresis. The hysteresis has a defined minimum (typ 5\%) and a maximum (typ 30\%). The frequency may deviate from nominal in some conditions. This depends upon the desired LED current, the coil inductance and the voltages at the input and the load. Loop compensation is achieved by a single external capacitor C 2 , connected between SHP and SGND.

The control loop sets the duty cycle so that the sense voltage is

$$
\mathrm{V}_{\mathrm{SENSE}}=0.218\left(\frac{\mathrm{~V}_{\mathrm{ADJ}}}{\mathrm{~V}_{\mathrm{REF}}}\right)
$$

Therefore,

$$
\text { LEED }=\left(\frac{0.218}{R_{S}}\right)\left(\frac{V_{\mathrm{ADJ}}}{\mathrm{~V}_{\mathrm{REF}}}\right) \text { (Buck mode) Equation } 1
$$

If the ADJ pin connected to the REF pin, this simplifies to

$$
\text { LLED }=\left(\frac{0.218}{\mathrm{R}_{\mathrm{S}}}\right)\left(\frac{\mathrm{V}_{\mathrm{ADJ}}}{\mathrm{~V}_{\mathrm{REF}}}\right)(\text { Buck mode })
$$



Figure 21 Buck Configuration


Figure 22 Operating Waveforms (Buck Mode)

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## Application Information (cont.)

## b) Boost and Buck-Boost modes - the most simple boost/buck-boost circuit is shown in Figure 23

Control in Boost and Buck-boost mode is achieved by sensing the coil current in the series resistor Rs, connected between the two inputs of a current monitor within the control loop block. An output from the control loop drives the input of a comparator which drives the gate of the external NMOS switch transistor Q1 via the internal Gate Driver. When the switch is on, the drain voltage of Q1 is near zero. Current flows from VIN, via Rs, coil and switch to ground. This current ramps up until an upper threshold value is reached (see Figure 24). At this point GATE goes low, the switch is turned off and the drain voltage increases to either:

1) the load voltage VLEDS plus the forward voltage of D1 in Boost configuration,
or
2) the load voltage VLEDS plus the forward voltage of D1 plus VIN in Buck-boost configuration.

Current flows via Rs, coil, D1 and LED back to VIN (Buck-boost mode), or GND (Boost mode). When the coil current has ramped down to a lower threshold value, GATE goes high, the switch is turned on again and the cycle of events repeats, resulting in continuous oscillation. The feeback loop adjusts the NMOS switch duty cycle to stabilize the LED current in response to changes in external conditions, including input voltage and load voltage. Loop compensation is achieved by a single external capacitor C2, connected between SHP and SGND. Note that in reality, a load capacitor Cout is used, so that the LED current waveform shown is smoothed.

The average current in the sense resistor and coil, IRs, is equal to the average of the maximum and minimum threshold currents and the ripple current (hysteresis) is equal to the difference between the thresholds.

The average current in the LED, lLeD, is always less than IRs. The feedback control loop adjusts the switch duty cycle, D , to achieve a set point at the sense resistor. This controls $\mathrm{I}_{\mathrm{RS}}$. During the interval toff, the coil current flows through D1 and the LED load. During ton, the coil current flows through Q1, not the LEDs. Therefore the set point is modified by D using a gating function to control ILED indirectly. In order to compensate internally for the effect of the gating function, a control factor, GI_ADJ is used. GI_ADJ is set by a pair of external resistors, $\mathrm{R}_{\mathrm{G} 11}$ and $\mathrm{R}_{\mathrm{G} 12}$. (Figure 23.) This allows the sense voltage to be adjusted to an optimum level for power efficiency without significant error in the LED controlled current.

$$
\mathrm{GI} \_\mathrm{ADJ}=\left(\frac{\mathrm{RGl} 1}{\mathrm{RGI} 1+\mathrm{RGI2}}\right)
$$

Equation 2 (Boost and Buck-boost modes)
The control loop sets the duty cycle so that the sense resistor current is

$$
\mathrm{R}_{\mathrm{S}}=\left(\frac{0.225}{\mathrm{RS}_{\mathrm{S}}}\right)\left(\frac{\mathrm{GI} \_\mathrm{ADJ}}{1-\mathrm{D}}\right)\left(\frac{\mathrm{V}_{\mathrm{ADJ}}}{\mathrm{~V}_{\mathrm{REF}}}\right)
$$

Equation 3 (Boost and Buck-boost modes)
$I_{R S}$ equals the coil current. The coil is connected only to the switch and the schottky diode. The schottky diode passes the LED current.


Figure 23 Boost and Buck-Boost Configuration


Figure 24 Operating Waveforms
(Boost and Buck-boost modes)

## Application Information (cont.)

Therefore the average LED current is the coil current multiplied by the schottky diode duty cycle, 1-D.
$\operatorname{ILED}=\operatorname{lRS}(1-\mathrm{D})=\left(\frac{0.225}{\mathrm{RS}_{S}}\right) G I_{-A D J}\left(\frac{\mathrm{~V}_{\mathrm{ADJ}}}{\mathrm{V}_{\mathrm{REF}}}\right)$
(Boost and Buck-Boost)
Equation 4

This shows that the LED current depends on the ADJ pin voltage, the reference voltage and 3 resistor values (RS, RGI1 and RGI2). It is independent of the input and output voltages.

If the ADJ pin is connected to the REF pin, this simplifies to
$\operatorname{LLED}=\left(\frac{0.225}{\mathrm{RS}_{S}}\right) \mathrm{GI} \_A D J$
(Boost and Buck-Boost)

Now led is dependent only on the 3 resistor values.
Considering power dissipation and accuracy, it is useful to know how the mean sense voltage varies with input voltage and other parameters.
$\mathrm{V}_{\mathrm{RS}}=\mathrm{I}_{\mathrm{RS}}=0.225\left(\frac{\mathrm{GI} \_\mathrm{ADJ}}{1-\mathrm{D}}\right)\left(\frac{\mathrm{V}_{\mathrm{ADJ}}}{\mathrm{V}_{\mathrm{REF}}}\right) \quad$ (Boost and Buck-Boost) Equation 5
This shows that the sense voltage varies with duty cycle in Boost and Buck-Boost configurations.

## Application Circuit Design

External component selection is driven by the characteristics of the load and the input supply, since this will determine the kind of topology being used for the system. Component selection begins with the current setting procedure, the inductor/frequency setting and the MOSFET selection. Finally after selecting the freewheeling diode and the output capacitor (if needed), the application section will cover the PWM dimming and thermal feedback. The full procedure is greatly accelerated by the web Calculator spreadsheet, which includes fully automated component selection, and is available on the Diodes web site. However the full calculation is also given here.

Some components depend upon the switching frequency and the duty cycle. The switching frequency is regulated by the ZXLD1370 to a large extent, depending upon conditions. This is discussed in a later paragraph dealing with coil selection.

## Duty Cycle Calculation and Topology Selection

The duty cycle is a function of the input and output voltages. Approximately, the MOSFET switching duty cycle is
$D_{\text {BUCK }} \approx \frac{\mathrm{V}_{\text {OUT }}}{\mathrm{V}_{\text {IN }}} \quad$ for Buck
$\mathrm{D}_{\text {BOOST }} \approx \frac{\mathrm{V}_{\text {OUT }}-\mathrm{V}_{\text {IN }}}{\mathrm{V}_{\text {OUT }}} \quad$ for Boost $\quad$ _
Equation 6
$\mathrm{D}_{\mathrm{BB}} \approx \frac{\mathrm{V}_{\text {OUT }}}{\mathrm{V}_{\text {OUT }}+\mathrm{V}_{\text {IN }}} \quad$ for Buck-Boost
Because D must always be a positive number less than 1 , these equations show that

$$
\begin{array}{lc}
V_{\text {OUT }}<\mathrm{V}_{\text {IN }} & \text { for Buck (voltage step-down) } \\
V_{\text {OUT }}>\mathrm{V}_{\text {IN }} & \text { for Boost (voltage step-up) } \\
V_{\text {OUT }}>\text { or }=\text { or }<\mathrm{V}_{\text {IN }} & \text { for Buck-boost (voltage step-down or step-up) }
\end{array}
$$

This allows us to select the topology for the required voltage range.

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## Application Information (cont.)

More exact equations are used in the web Calculator. These are:

|  | $\mathrm{D}_{\text {BUCK }}=\frac{\mathrm{V}_{\text {OUT }}+\mathrm{V}_{\mathrm{F}}+\mathrm{l}_{\text {OUT }}\left(\mathrm{R}_{\mathrm{S}}+\mathrm{R}_{\text {COIL }}\right)}{\mathrm{V}_{\text {IN }}+\mathrm{V}_{\mathrm{F}}-\mathrm{V}_{\text {DSON }}}$ | for Buck |  |
| :---: | :---: | :---: | :---: |
|  | $\mathrm{D}_{\text {BOOST }}=\frac{\mathrm{V}_{\text {OUT }}-\mathrm{V}_{\text {IN }}+\mathrm{l}_{\text {IN }}\left(\mathrm{R}_{\mathrm{S}}+\mathrm{R}_{\text {COIL }}\right)+\mathrm{V}_{\mathrm{F}}}{\mathrm{~V}_{\text {OUT }}+\mathrm{V}_{\mathrm{F}}-\mathrm{V}_{\text {DSON }}}$ | for Boost | Equation 7 |
|  | $\mathrm{D}_{\mathrm{BB}}=\frac{\mathrm{V}_{\mathrm{OUT}}+\mathrm{V}_{\mathrm{F}}+\left(\mathrm{l}_{\mathrm{IN}}+\mathrm{l}_{\mathrm{OUT}}\right)\left(\mathrm{R}_{\mathrm{S}}+\mathrm{R}_{\mathrm{COIL}}\right)}{\mathrm{V}_{\text {OUT }}+\mathrm{V}_{\text {IN }}+\mathrm{V}_{\mathrm{F}}-\mathrm{V}_{\mathrm{DSON}}}$ | for Buck-boost |  |
| where | $V_{F} \quad=$ schottky diode forward voltage, estim | ted for the expe |  |
|  | $V_{\text {DSON }}=$ MOSFET drain source voltage in the | ON condition (de | rain current |
|  | $\mathrm{R}_{\text {COIL }}=$ DC winding resistance of L1 |  |  |

The additional terms are relatively small, so the exact equations will only make a significant difference at lower operating voltages at the input and output, i.e. low input voltage or a small number of LEDs connected in series. The estimates of $\mathrm{V}_{\mathrm{F}}$ and $\mathrm{V}_{\mathrm{Ds}}$. depend on the coil current. The mean coil current, ICOIL depends upon the topology and upon the mean terminal currents as follows:

$$
I_{\text {COIL }}=\left\{\begin{array}{ll}
I_{\text {LED }} & \text { for Buck } \\
I_{I N} & \text { for Boost } \\
I_{I N}+I_{\text {LED }} & \text { for Buck-boost }
\end{array} \quad \text { Equation } 8\right.
$$

ILED is the target LED current and is already known. I IN will be calculated with some accuracy later, but can be estimated now from the electrical power efficiency. If the expected efficiency is roughly $90 \%$, the output power Pout is $90 \%$ of the input power, PIN, and the coil current is estimated as follows.

$$
\begin{array}{ll} 
& \text { POUT } \\
\text { or } & \approx 0.9 \mathrm{P}_{\mathrm{IN}} \\
\mathrm{I}_{\text {LED }} N V_{\text {LED }} & \approx 0.9 \mathrm{I}_{\mathrm{IN}} \mathrm{~V}_{\mathrm{IN}}
\end{array}
$$

where N is the number of LEDs connected in series, and $\mathrm{V}_{\text {LED }}$ is the forward voltage drop of a single LED at led.
So $\quad \mathrm{I}_{\mathrm{IN}} \approx \frac{\mathrm{L}_{\mathrm{LED}} N \mathrm{~V}_{\mathrm{LED}}}{0.9 \mathrm{~V}_{\mathrm{IN}}}$

## Equation 9

Equation 9 can now be used to find $\mathrm{I}_{\text {COIL }}$ in Equation 8, which can then be used to estimate the small terms in Equation 7. This completes the calculation of Duty Cycle and the selection of Buck, Boost or Buck-boost topology.

An initial estimate of duty cycle is required before we can choose a coil. In Equation 7, the following approximations are recommended:

| $V_{F}$ | $=0.5 \mathrm{~V}$ |
| :---: | :---: |
| $\mathrm{IIN}^{\left(R_{S}+R_{\text {coil }}\right)}$ | $=0.5 \mathrm{~V}$ |
| lout $\mathrm{R}_{\text {S }}+\mathrm{R}_{\text {COIL }}$ ) | $=0.5 \mathrm{~V}$ |
| $\mathrm{V}_{\text {DSON }}$ | $=0.1 \mathrm{~V}$ |
| $\left(\mathrm{l}_{\text {N }}+\mathrm{l}_{\text {OUT }}\right)\left(\mathrm{R}_{\text {S }}+\mathrm{R}_{\text {COIL }}\right)$ | $=1.1 \mathrm{~V}$ |

## Then Equation 7 becomes

$$
\begin{aligned}
& \mathrm{D}_{\text {BUCK }} \approx \frac{\mathrm{V}_{\text {OUT }}+1}{\mathrm{~V}_{\text {IN }}+0.4} \\
& \mathrm{D}_{\text {BOOST }} \approx \frac{\mathrm{V}_{\text {OUT }}-\mathrm{V}_{\text {IN }}+1}{\mathrm{~V}_{\text {OUT }}+0.4} \\
& \mathrm{D}_{\mathrm{BB}} \approx \frac{\mathrm{~V}_{\text {OUT }}+1.6}{\mathrm{~V}_{\text {OUT }}+\mathrm{V}_{\text {IN }}+0.4}
\end{aligned}
$$



Equation 7a

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## Application Information (cont.)

## Setting the LED current

The LED current requirement determines the choice of the sense resistor Rs. This also depends on the voltage on the ADJ pin and the voltage on the Gl pin, according to the topology required.

The ADJ pin may be connected directly to the internal 1.25 V reference ( $\mathrm{V}_{\mathrm{REF}}$ ) to define the nominal $100 \%$ LED current. The ADJ pin can also be driven with an external dc voltage between 125 mV and 2.5 V to adjust the LED current proportionally between $10 \%$ and $200 \%$ of the nominal value.

For a divider ratio GI_ADJ greater than 0.65 V , the ZXLD 1370 operates in Buck mode when $\mathrm{V}_{\text {ADJ }}=1.25 \mathrm{~V}$. If $\mathrm{GI} \_\mathrm{ADJ}$ is less than 0.65 V (typical), the device operates in Boost or buck-Boost mode, according to the load connection. This 0.65 V threshold varies in proportion to $\mathrm{V}_{\mathrm{ADJ}}$, i.e., the Buck mode threshold voltage is $0.65 \mathrm{~V}_{\mathrm{ADJ}} / 1.25 \mathrm{~V}$.

ADJ and Gl are high impedance inputs within their normal operating voltage ranges. An internal 2.6 V clamp protects the device against excessive input voltage and limits the maximum output current to approximately $4 \%$ above the maximum current set by $\mathrm{V}_{\mathrm{REF}}$ if the maximum input voltage is exceeded.

## Buck Topology

In Buck mode, GI is connected to ADJ as in Figure 25. The LED current depends only upon $R_{S}, V_{A D J}$ and $V_{R E F}$. From Equation 1 above,

$$
\mathrm{RsBUCK}=\left(\frac{0.218}{\operatorname{lLED}}\right)\left(\frac{\mathrm{V}_{\mathrm{ADJ}}}{\mathrm{~V}_{\mathrm{REF}}}\right)
$$

## Equation 10

If ADJ is directly connected to VREF, this becomes:

$$
\mathrm{R}_{\text {SBUCK }}=\left(\frac{0.218}{\operatorname{lLED}}\right)
$$



Figure 25 Setting LED Current in Buck Configuration

## Boost and Buck-Boost Topology

For Boost and Buck-boost topologies, the LED current depends upon the resistors, $\mathrm{R}_{\mathrm{S}}$, $\mathrm{R}_{\mathrm{G} 11}$, and $\mathrm{R}_{\mathrm{G} \mid 2}$ as in Equations 4 and 2 above. There is more than one degree of freedom. That is to say, there is not a unique solution. From Equation 4,

$$
\mathrm{R}_{\text {SBOOSTBB }}=\left(\frac{0.225}{\text { LEED }}\right) \mathrm{GI} \_ \text {ADJ }\left(\frac{\mathrm{V}_{\text {ADJ }}}{\mathrm{V}_{\text {REF }}}\right) \quad \text { Equation } 11
$$

If ADJ is connected to REF, this becomes

$$
\mathrm{RSBOOSTBB}=\left(\frac{0.225}{\operatorname{lLED}}\right) \mathrm{GI} \_\mathrm{ADJ}
$$

GI_ADJ is given by Equation 2, repeated here for convenience:

$$
\mathrm{GI} \_\mathrm{ADJ}=\left(\frac{\mathrm{RGl} 1}{\mathrm{RGl1}+\mathrm{RGI} 2}\right)
$$

Note that from considerations of ZXLD1370 input bias current, the recommended limits for $\mathrm{R}_{\mathrm{G} 11}$ are:

$$
22 \mathrm{k} \Omega<\mathrm{R}_{\mathrm{Gl} 1}<100 \mathrm{k} \Omega
$$

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ZXLD1370

## Application Information (cont.)

The additional degree of freedom allows us to select GI_ADJ within limits but this may affect overall performance a little. As mentioned above, the working voltage range at the GI pin is restricted. The permitted range of GI ADJ in Boost or Buck-boost configuration is

$$
0.2<\text { GI_ADJ < } 0.5 \quad \text { Equation } 13
$$

The mean voltage across the sense resistor is

$$
\mathrm{V}_{\mathrm{RS}}=\mathrm{I}_{\mathrm{COIL}} \mathrm{R}_{\mathrm{S}}
$$

Equation 14

Note that if GI_ADJ is made larger, these equations show that $R_{S}$ is increased and $V_{R S}$ is increased. Therefore, for the same coil current, the dissipation in $R_{S}$ is increased. So, in some cases, it is better to minimize GI_ADJ. However, consider Equation 5. If ADJ is connected to REF, this becomes

$$
\mathrm{V}_{\mathrm{RS}}=0.225\left(\frac{\mathrm{GI} \_\mathrm{ADJ}}{1-\mathrm{D}}\right)
$$

This shows that $V_{R S}$ becomes smaller than $225 m V$ if $G I \_A D J<1-D$. If also $D$ is small, $V_{R S}$ can become too small. For example if $D=0.2$, and GI_ADJ is the minimum value of 0.2 , then $V_{R S}$ becomes $0.225^{*} 0.2 / 0.8=56.25 \mathrm{mV}$. This will increase the LED current error due to small offsets in the system, such as mV drop in the copper printed wiring circuit, or offset uncertainty in the ZXLD1370. If now, GI_ADJ is increased to 0.4 or $0.5, \mathrm{~V}_{\mathrm{RS}}$ is increased to a value greater than 100 mV . This will give small enough l $\mathrm{l}_{\text {LED }}$ error for most practical purposes. Satisfactory operation will be obtained if $\mathrm{V}_{R S}$ is more than about 80 mV . This means GI_ADJ should be greater than (1-DMIN)* $80 / 225=\left(1-D_{\text {MIN }}\right) * 0.355$.

There is also a maximum limit on $V_{R S}$ which gives a maximum limit for GI_ADJ. If $V_{R S}$ exceeds approximately 300 mV , or $133 \%$ of 225 mV , the STATUS output may indicate an over-current condition. This will happen for larger $\mathrm{D}_{\mathrm{MAX}}$.

Therefore, together with the requirement of Equation 13, the recommended range for GI_ADJ is

$$
0.355\left(1-\mathrm{D}_{\mathrm{MIN}}\right)<\mathrm{GI} A D J<1.33\left(1-\mathrm{D}_{\mathrm{MAX}}\right)
$$

Equation 15
An optimum compromise for GI_ADJ has been suggested, i.e.

$$
\mathrm{GI}_{\text {AD }}^{\text {AUTO }}=1-\mathrm{D}_{\text {MAX }}
$$

Equation 16
This value has been used for the "Automatic" setting of the web Calculator. If $1-D_{\text {mAx }}$ is less than 0.2 , then GI_ADJ is set to 0.2 . If $1-D_{\text {MAX }}$ is greater than 0.5 then GI_ADJ is set to 0.5

Once GI_ADJ has been selected, a value of RGI1 can be selected from Equation 12.
Then RGI2 is calculated as follows, rearranging Equation 2:

$$
R_{G 12}=R_{G 11}\left(\frac{1-\mathrm{GI}_{-} \mathrm{ADJ}}{\mathrm{GI}-\mathrm{ADJ}}\right) \quad \text { Equation } 17
$$

For example to drive 12 LEDS at a current of 350 mA from a 12 V supply requires Boost configuration. Each LED has a forward voltage of 3.2 V at 350 mA , so Vout $=3.2 * 12=38.4 \mathrm{~V}$. From Equation 6, the duty cycle is approximately

$$
\frac{\left(\text { VOUT- }_{\text {IIN }}\right)}{V_{\text {OUT }}}=\left(\frac{38.4-12}{38.4}\right)=0.6875
$$

From Equation 16, we set GI_ADJ to 1 - D = 0.3125.
IF $R_{G I 1}=33 k \Omega$, then from Equation 17,

$$
\mathrm{R}_{\mathrm{G} 12}=33 \times\left(\frac{1-0.3125}{0.3125}\right)=72.6 \mathrm{k} \Omega
$$

Let us choose the preferred value $R_{G l 2}=75 \mathrm{k} \Omega$. Now GI_ADJ is adjusted to the new value, using Equation 2.

$$
\mathrm{GI} \_\mathrm{ADJ}=\left(\frac{\mathrm{RGI1}}{\mathrm{RGI1}+\mathrm{RGI2}}\right)=\frac{33 \mathrm{k}}{33 \mathrm{k}+75 \mathrm{k}}=0.305
$$

## Application Information (cont.)

Now we calculate Rs from Equation 11. Assume ADJ is connected to REF.
$R_{\text {SBOOSTBB }}=\left(\frac{0.225}{\operatorname{lLED}}\right) \times G I_{-A D J x}\left(\frac{V_{\text {ADJ }}}{V_{\text {REF }}}\right)=\frac{0.225}{0.35} \times 0.305=0.196 \Omega$
A preferred value of $R_{\text {SBoostBB }}=0.2 \Omega$ will give the desired LED current with an error of $2 \%$ due to the preferred value selection.
Table 1 shows typical resistor values used to determine the GI_ADJ ratio with E24 series resistors
Table 1

| GI ratio | RGI1 | RG2 |
| :---: | :---: | :---: |
| 0.2 | $30 \mathrm{k} \Omega$ | $120 \mathrm{k} \Omega$ |
| 0.25 | $33 \mathrm{k} \Omega$ | $100 \mathrm{k} \Omega$ |
| 0.3 | $39 \mathrm{k} \Omega$ | $91 \mathrm{k} \Omega$ |
| 0.35 | $30 \mathrm{k} \Omega$ | $56 \mathrm{k} \Omega$ |
| 0.4 | $100 \mathrm{k} \Omega$ | $150 \mathrm{k} \Omega$ |
| 0.45 | $51 \mathrm{k} \Omega$ | $62 \mathrm{k} \Omega$ |
| 0.5 | $30 \mathrm{k} \Omega$ | $30 \mathrm{k} \Omega$ |

This completes the LED current setting.

## Inductor Selection and Frequency Control

The selection of the inductor coil, L1, requires knowledge of the switching frequency and current ripple, and also depends on the duty cycle to some extent. In the hysteretic converter, the frequency depends upon the input and output voltages and the switching thresholds of the current monitor. The peak-to-peak coil current is adjusted by the ZXLD1370 to control the frequency to a fixed value. This is done by controlling the switching thresholds within particular limits. This effectively much reduces the overall frequency range for a given input voltage range. Where the input voltage range is not excessive, the frequency is regulated to approximately 330 kHz in Buck configuration, and 300 kHz in Boost and Buck-boost configurations. This is helpful in terms of EMC and other system requirements.

For larger input voltage variation, or when the choice of coil inductance is not optimum, the switching frequency may depart from the regulated value, but the regulation of LED current remains successful. If desired, the frequency can to some extent be increased by using a smaller inductor, or decreased using a larger inductor. The web Calculator will evaluate the frequency across the input voltage range and the effect of this upon power efficiency and junction temperatures.

Determination of the input voltage range for which the frequency is regulated may be required. This calculation is very involved, and is not given here. However the performance in this respect can be evaluated within the web Calculator for the chosen inductance.

The inductance is given as follows in terms of peak-to-peak ripple current in the coil, $\Delta \mathrm{I}_{\mathrm{L}}$ and the MOSFET on time, $t_{0 N}$.

Therefore In order to calculate L 1 , we need to find $\mathrm{I}_{\mathrm{N}}$, $\mathrm{t}_{\mathrm{N}}$, and $\Delta \mathrm{I}_{\mathrm{L}}$. The effects of the resistances are small and will be estimated.
$I_{\mathbb{N}}$ is estimated from Equation 9.

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## Application Information (cont.)

$t_{O N}$ is related to switching frequency, $f$, and duty cycle, $D$, as follows:

$$
\operatorname{toN}=\frac{D}{f}
$$

## Equation 19

As the regulated frequency is known, and we have already found D from Equation $\mathbf{7}$ or the approximation Equation $\mathbf{7 b}$, this allows calculation of ton.

The ZXLD1370 sets the ripple current, $\Delta I_{L}$ is monitored by the ZXLD1370 which sets this to be between nominally $10 \%$ and $30 \%$ of the mean coil current, Icoll, which is found from Equation 8. The device adjusts the ripple current within this range in order to regulate the switching frequency. We therefore need to use a value of $20 \%$ of $I_{\text {coll }}$ to find an inductance which is optimized for the input voltage range. The range of ripple current control is also modulated by other circuit parameters as follows.

$$
\begin{aligned}
& \Delta l_{\text {LMAX }}=\left\{0.03+0.12\left(\frac{V_{\text {ADJ }}}{V_{R E F}}\right)\right\} \frac{1-D}{G I_{\_A D J}} I_{\text {COIL }} \\
& \Delta \mathrm{ILMIN}=\left\{0.01+0.04\left(\frac{\mathrm{~V}_{\text {ADJ }}}{\mathrm{V}_{\text {REF }}}\right)\right\} \frac{1-\mathrm{D}}{\mathrm{GI}_{\_} \mathrm{ADJ}} \mathrm{l} \text { coIL } \\
& \Delta \mathrm{L}_{\mathrm{LMID}}=\left\{0.02+0.08\left(\frac{\mathrm{~V}_{\text {ADJ }}}{V_{\text {REF }}}\right)\right\} \frac{1-\mathrm{D}}{\mathrm{GI} \_ \text {ADJ }} \mathrm{l}_{\mathrm{COIL}}
\end{aligned}
$$



Equation 20

If $A D J$ is connected to REF, this simplifies to

$$
\begin{aligned}
& \Delta \text { lımAX }=0.15 \frac{1-\mathrm{D}}{\mathrm{GI} \_ \text {ADJ }} \mathrm{I}_{\text {coil }} \\
& \Delta \text { LLMIN }=0.05 \frac{1-\mathrm{D}}{\mathrm{GI} \_\mathrm{ADJ}} \mathrm{l}_{\mathrm{COIL}} \\
& \Delta \mathrm{ILMID}=0.1 \frac{1-\mathrm{D}}{\mathrm{GI} \text { ADJ }} \mathrm{I}_{\mathrm{COIL}}
\end{aligned}
$$



Equation 20a
where $\Delta_{\text {LMID }}$ is the value we must use in Equation 18. We have now established the inductance value.
The chosen coil should have a saturation current higher than the peak sensed current. This saturation current is the DC current for which the inductance has decreased by $10 \%$ compared to the low current value.

Assuming $\pm 10 \%$ ripple current, we can find this peak current from Equation 8, adjusted for ripple current:

$$
I_{\text {COILPEAK }}=\left\{\begin{array}{ll}
1.1 \mathrm{I}_{\mathrm{LED}} & \text { for Buck } \\
1.1 \mathrm{I}_{\mathrm{INMAX}} & \text { for Boost } \\
1.1 \mathrm{I}_{\mathrm{INMAX}}+I_{\text {LED }} & \text { for Buck-boost }
\end{array} \quad \text { Equation } 21\right.
$$

where $l_{I N M A X}$ is the value of $I_{I N}$ at minimum $V_{I N}$.
The mean current rating is also a factor, but normally the saturation current is the limiting factor.

The following websites may be useful in finding suitable components
www.coilcraft.com
www.niccomp.com
www.wuerth-elektronik.de

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## Application Information (cont.)

## MOSFET Selection

The ZXLD1370 requires an external NMOS FET as the main power switch with a voltage rating at least $15 \%$ higher than the maximum circuit voltage to ensure safe operation during the overshoot and ringing of the switch node. The current rating is recommended to be at least $10 \%$ higher than the average transistor current. The power rating is then verified by calculating the resistive and switching power losses.

$$
\text { P = PRESISTIVE }+ \text { PSWITCHING }
$$

## Resistive Power Losses

The resistive power losses are calculated using the RMS transistor current and the MOSFET on-resistance.
Calculate the current for the different topologies as follows:

## Buck Mode

$$
\mathrm{I}_{\text {MOSFET-MAX }}=\mathrm{D}_{\mathrm{MAX}} \times \mathrm{I}_{\text {LED }}
$$

## Boost / Buck-Boost Mode

$$
l_{\text {MOSFET }- \text { MAX }}=\frac{D_{M A X}}{1-D_{M A X}} \times i_{L E D}
$$

The approximate RMS current in the MOSFET will be:

## Buck Mode

$$
I_{\text {MOSFET -RMS }}=I_{\text {LED }} \sqrt{D}
$$

## Boost / Buck-Boost Mode

$$
I_{\text {MOSFET -RMS }}=\frac{\sqrt{D}}{1-D} \times I_{\text {LED }}
$$

The resistive power dissipation of the MOSFET is:

$$
\mathrm{P}_{\text {RESISTIVE }}=\mathrm{I}_{\text {MOSFET-RMS }}{ }^{2} \times \mathrm{R}_{\text {DS-ON }}
$$

## Switching Power Losses

Calculating the switching MOSFET's switching loss depends on many factors that influence both turn-on and turn-off. Using a first order rough approximation, the switching power dissipation of the MOSFET is:

$$
P_{\text {SWITCHING }}=\frac{C_{R S S} \times V^{2}{ }_{I N} \times f_{S W} \times I_{\text {LOAD }}}{I_{\text {GATE }}}
$$

where
$\mathrm{C}_{\mathrm{RSS}}$ is the MOSFET's reverse-transfer capacitance (a data sheet parameter),
fsw is the switching frequency,
$I_{\text {GATE }}$ is the MOSFET gate-driver's sink/source current at the MOSFET's turn-on threshold.

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## Application Information (cont.)

Matching the MOSFET with the controller is primarily based on the rise and fall time of the gate voltage. The best rise/fall time in the application is based on many requirements, such as EMI (conducted and radiated), switching losses, lead/circuit inductance, switching frequency, etc. How fast a MOSFET can be turned on and off is related to how fast the gate capacitance of the MOSFET can be charged and discharged. The relationship between $C$ (and the relative total gate charge Qg ), turn-on/turn-off time and the MOSFET driver current rating can be written as:

$$
\mathrm{dt}=\frac{\mathrm{dV} \cdot \mathrm{C}}{\mathrm{l}}=\frac{\mathrm{Qg}}{\mathrm{l}}
$$

where
dt = turn-on/turn-off time
dV = gate voltage
$\mathrm{C}=$ gate capacitance $=\mathrm{Qg} / \mathrm{V}$
I = drive current - constant current source (for the given voltage value)
Here the constant current source" $\mid$ " usually is approximated with the peak drive current at a given driver input voltage.
(Example 1)
Using the DMN6068 MOSFET $\left(\mathrm{V}_{\mathrm{DS}(\mathrm{MAX})}=60 \mathrm{~V}, \mathrm{I}_{\mathrm{D}(\mathrm{MAX})}=8.5 \mathrm{~A}\right)$ :

$$
\rightarrow Q_{G}=10.3 n C \text { at } V_{G S}=10 \mathrm{~V}
$$

ZXLD1370 IPEAK $=I_{\text {GATE }}=300 \mathrm{~mA}$

$$
\mathrm{dt}=\frac{\mathrm{Q}_{\mathrm{g}}}{I_{\text {PEAK }}}=\frac{10.3 \mathrm{nC}}{300 \mathrm{~mA}}=35 \mathrm{~ns}
$$

Assuming that cumulatively the rise time and fall time can account for a maximum of $10 \%$ of the period, the maximum frequency allowed in this condition is:

$$
t_{\text {PERIOD }}=20^{*} \mathrm{dt} \quad \rightarrow \quad \mathrm{f}=1 / \mathrm{t}_{\text {PERIOD }}=1.43 \mathrm{MHz}
$$

This frequency is well above the max frequency the device can handle, therefore the DNM6068 can be used with the ZXLD1370 in the whole spectrum of frequencies recommended for the device (from 300 kHz to 1 MHz ).
(Example 2)
Using the $\mathrm{ZXMN6A09K}\left(\mathrm{~V}_{\mathrm{DS}(\mathrm{MAX})}=60 \mathrm{~V}, \mathrm{I}_{\mathrm{D}(\mathrm{MAX})}=12.2 \mathrm{~A}\right)$ :

$$
\rightarrow Q_{G}=29 \mathrm{nC} \text { at } V_{G S}=10 \mathrm{~V}
$$

ZXLD 1370 IPEAK $=300 \mathrm{~mA}$

$$
\mathrm{dt}=\frac{\mathrm{Q}_{\mathrm{g}}}{\mathrm{I}_{\text {PEAK }}}=\frac{29 \mathrm{nC}}{300 \mathrm{~mA}}=97 \mathrm{~ns}
$$

Assuming that cumulatively the rise time and fall time can account for a maximum of $10 \%$ of the period, the maximum frequency allowed in this condition is:

$$
\text { tPERIOD }=20^{*} \mathrm{dt} \quad \rightarrow \quad f=1 / \text { tPERIOD }=515 \mathrm{kHz}
$$

This frequency is within the recommended frequency range the device can handle, therefore the ZXMN6A09K is recommended to be used with the ZXLD1370 for frequencies from 300 kHz to 500 kHz ).
The recommended total gate charge for the MOSFET used in conjunction with the ZXLD1370 is less than 30nC.

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## Application Information (cont.)

## Junction Temperature Estimation

Finally, the ZXLD1370 junction temperature can be estimated using the following equations:
Total supply current of ZXLD1370:

$$
\mathrm{I}_{\mathrm{QTOT}} \approx \mathrm{I}_{\mathrm{Q}}+\mathrm{f} \cdot \mathrm{Q}_{\mathrm{G}}
$$

Where $I_{Q}=$ total quiescent current $I_{Q-I N}+I_{Q-A U X}$
Power consumed by ZXLD1370

$$
P_{\text {IC }}=V_{\text {IN }} \cdot\left(I_{Q}+f \cdot Q g\right)
$$

Or in case of separate voltage supply, with $\mathrm{V}_{\mathrm{A}} \mathrm{X}<15 \mathrm{~V}$

$$
\begin{aligned}
& P_{\mathrm{IC}}=\mathrm{V}_{\mathrm{IN}} \cdot \mathrm{I}_{\mathrm{Q}-\mathrm{IN}}+\mathrm{V}_{\mathrm{aux}} \cdot\left(\mathrm{I}_{\mathrm{Q}-\mathrm{AUX}}+\mathrm{f} \cdot \mathrm{Qg}\right) \\
& \mathrm{T}_{\mathrm{J}}=\quad \mathrm{T}_{\mathrm{A}}+\mathrm{P}_{\mathrm{IC}} \cdot \theta_{\mathrm{JA}}=\mathrm{T}_{\mathrm{A}}+\mathrm{P}_{\mathrm{IC}} \cdot\left(\theta_{\mathrm{JC}}+\theta_{\mathrm{CA}}\right)
\end{aligned}
$$

Where the total quiescent current $\mathrm{IQ}_{\text {TOT }}$ consists of the static supply current $(I Q)$ and the current required to charge and discharge the gate of the power MOSFET. Moreover the part of thermal resistance between case and ambient depends on the PCB characteristics.


Figure 27 Power Derating Curve for ZXLD1370 Mounted on Test Board According to JESD51

## Application Information (cont.)

## Diodes Selection

For maximum efficiency and performance, the rectifier (D1) should be a fast low capacitance Schottky diode* with low reverse leakage at the maximum operating voltage and temperature. The Schottky diode also provides better efficiency than silicon PN diodes, due to a combination of lower forward voltage and reduced recovery time.

It is important to select parts with a peak current rating above the peak coil current and a continuous current rating higher than the maximum output load current. In particular, it is recommended to have a voltage rating at least $15 \%$ higher than the maximum transistor voltage to ensure safe operation during the ringing of the switch node and a current rating at least $10 \%$ higher than the average diode current. The power rating is verified by calculating the power loss through the diode.

The higher forward voltage and overshoot due to reverse recovery time in silicon diodes will increase the peak voltage on the Drain of the external MOSFET. If a silicon diode is used, care should be taken to ensure that the total voltage appearing on the Drain of the external MOSFET, including supply ripple, does not exceed the specified maximum value.
*A suitable Schottky diode would be PDS3100 (Diodes Inc).

## Output Capacitor

An output capacitor may be required to limit interference or for specific EMC purposes. For boost and buck-boost regulators, the output capacitor provides energy to the load when the freewheeling diode is reverse biased during the first switching subinterval. An output capacitor in a buck topology will simply reduce the LED current ripple below the inductor current ripple. In other words, this capacitor changes the current waveform through the LED(s) from a triangular ramp to a more sinusoidal version without altering the mean current value.

In all cases, the output capacitor is chosen to provide a desired current ripple of the LED current (usually recommended to be less than $40 \%$ of the average LED current).

## Buck:

$$
\mathrm{C}_{\text {OUTPUT }}=\frac{\Delta \mathrm{I}_{\text {L-PP }}}{8 \times \mathrm{f}_{\text {SW }} \times r_{\text {LED }} \times \Delta \mathrm{I}_{\text {LED-PP }}}
$$

## Boost and Buck-Boost

$$
\mathrm{C}_{\text {OUTPUT }}=\frac{\mathrm{DxI}_{\text {LED-PP }}}{\mathrm{f}_{\mathrm{SW}} \times \mathrm{r}_{\text {LED }} \times \Delta \mathrm{I}_{\mathrm{LED}-\mathrm{PP}}}
$$

where:

- $\Delta \mathrm{l}_{\text {L-PP }}$ is the ripple of the inductor current, usually $\pm 20 \%$ of the average sensed current
- $\quad$ l $_{\text {LED-PP }}$ is the ripple of the LED current, it should be $<40 \%$ of the LEDs average current
- $f_{s w}$ is the switching frequency (From graphs and calculator)
- rLED is the dynamic resistance of the LEDs string ( n times the dynamic resistance of the single LED from the datasheet of the LED manufacturer).
The output capacitor should be chosen to account for derating due to temperature and operating voltage. It must also have the necessary RMS current rating. The minimum RMS current for the output capacitor is calculated as follows:


## Buck

$$
\mathrm{I}_{\text {COUTPUT-RMS }}=\frac{\mathrm{I}_{\mathrm{LED}-\mathrm{PP}}}{\sqrt{12}}
$$

## Boost and Buck-Boost

$$
\mathrm{I}_{\text {COUTPUT-RMS }}=\mathrm{I}_{\text {LED }} \sqrt{\frac{\mathrm{D}_{\text {MAX }}}{1-\mathrm{D}_{\text {MAX }}}}
$$

Ceramic capacitors with X7R dielectric are the best choice due to their high ripple current rating, long lifetime, and performance over the voltage and temperature ranges.

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## Application Information (cont.)

## Input Capacitor

The input capacitor can be calculated knowing the input voltage ripple $\Delta \mathrm{V}_{\mathbb{I N}-\mathrm{PP}}$ as follows:
Buck

$$
C_{I N}=\frac{D x(1-D) x I_{\text {LED }}}{f_{S W} \times \Delta V_{I N-P P}} \quad \text { Use } D=0.5 \text { as worst case }
$$

Boost

$$
\mathrm{C}_{\mathrm{IN}}=\frac{\Delta \mathrm{I}_{\mathrm{L}-\mathrm{PP}}}{8 \mathrm{x} \mathrm{f}_{\mathrm{SW}} \times \Delta \mathrm{V}_{\mathrm{IN}-\mathrm{PP}}}
$$

## Buck-Boost

$$
\mathrm{C}_{\mathrm{IN}}=\frac{\mathrm{D} \times \mathrm{I}_{\mathrm{LED}}}{\mathrm{f}_{\mathrm{SW}} \times \Delta \mathrm{V}_{\mathrm{IN}-\mathrm{PP}}} \quad \text { Use } \mathrm{D}=\mathrm{D}_{\mathrm{MAX}} \text { as worst case }
$$

The minimum RMS current for the output capacitor is calculated as follows:
Buck

$$
I_{C I N-R M S}=I_{\text {LED }} \times \sqrt{D x(1-D)} \quad \text { use } D=0.5 \text { as worst case }
$$

Boost

$$
\mathrm{I}_{\mathrm{CIN}-\mathrm{RMS}}=\frac{\mathrm{I}_{\mathrm{L}-\mathrm{PP}}}{\sqrt{12}}
$$

## Buck-Boost

$$
\mathrm{I}_{\mathrm{CIN}-\mathrm{RMS}}=\mathrm{I}_{\mathrm{LED}} \mathrm{X} \sqrt{\frac{\mathrm{D}}{(1-\mathrm{D})}} \quad \text { Use } \mathrm{D}=\mathrm{D}_{\mathrm{MAX}} \text { as worst case }
$$

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## Application Information (cont.)

## PWM Output Current Control \& Dimming

The ZXLD1370 has a dedicated PWM dimming input that allows a wide dimming frequency range from 100 Hz to 1 kHz with up to $1000: 1$ resolution; however higher dimming frequencies can be used - at the expense of dimming dynamic range and accuracy.

Typically, for a PWM frequency of 1 kHz , the error on the current linearity is lower than $5 \%$; in particular the accuracy is better than $1 \%$ for PWM from $5 \%$ to $100 \%$. This is shown in the graph below:


Figure 28 LED Current Linearity and Accuracy with PWM Dimming at $\mathbf{1 k H z}$
For a PWM frequency of 100 Hz , the error on the current linearity is lower than $2.5 \%$; it becomes negligible for PWM greater than $5 \%$. This is shown in the graph below:


Figure 29 LED Current Linearity and Accuracy with PWM Dimming at 100Hz
The PWM pin is designed to be driven by both 3.3 V and 5 V logic levels. It can be driven also by an open drain/collector transistor. In this case the designer can either use the internal pull-up network or an external pull-up network in order to speed-up PWM transitions, as shown in the Boost/ Buck-Boost section.

ZXLD1370

## Application Information (cont.)



Figure 30. PWM Dimming from Open Collector Switch


Figure 31 PWM Dimming from MCU


Figure 32 PWM Dimming Minimum and Maximum Pulse

LED current can be adjusted digitally, by applying a low frequency PWM logic signal to the PWM pin to turn the controller on and off. This will produce an average output current proportional to the duty cycle of the control signal. During PWM operation, the device remains powered up and only the output switch is gated by the control signal.

The PWM signal can achieve very high LED current resolution. In fact, dimming down from $100 \%$ to $0.1 \%$ at 500 Hz , a minimum pulse width of $2 \mu \mathrm{~s}$ can be achieved resulting in very high resolution and accuracy. While the maximum recommended pulse is for the PWM signal is 10ms (equivalent to 100 Hz ) See Figure 32.

The ultimate PWM dimming ratio will be determined by the switching frequency as the minimum PWM pulse width is determined by resolving at least 1 switching cycle. The figure to the right the switching waveforms for a low duty cycle PWM dimming.

As can be seen, when the LED current restarts (blue waveform) it has to start all the way from zero to the peak level set by $\mathrm{V}_{\text {SENSE }} / \mathrm{R}_{\mathrm{S}}{ }^{* 1.15 \text {. So the first pulse is always longer than the }}$ nominal switching frequency would imply.



The PWM pin can be used to put the device into standby. Taking the PWM pin low ( $<0.4 \mathrm{~V}$ ) for more than 25 ms (typically 15 ms ) the device will enter its standby state and most of the internal circuitry is switched off and residual quiescent current will be typically $90 \mu \mathrm{~A}$. In particular, the Status pin will go down to GND while the FLAG and REF pins will stay at their nominal values.

Figure 33 Standby State from PWM signal
When the device restarts from standby mode, a "start-up" time must be allowed for before the device resume full LED current regulation.

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## Application Information (cont.)

## Thermal Control of LED Current

For thermal control of the LEDs, the ZXLD1370 monitors the voltage on the TADJ pin and reduces output current if the voltage on this pin falls below 625 mV . An external NTC thermistor and resistor can therefore be connected as shown below to set the voltage on the TADJ pin to 625 mV at the required temperature threshold. This will give $100 \%$ LED current below the threshold temperature and a falling current above it as shown in the graph. The temperature threshold can be altered by adjusting the value of Rth and/or the thermistor to suit the requirements of the chosen LED.

The Thermal Control feature can be disabled by connecting TADJ directly to REF.
Here is a simple procedure to design the thermal feedback circuit:

1) Select the temperature threshold $T_{\text {threshold }}$ at which the current must start to decrease
2) Select the Thermistor TH 1 (both resistive value at $+25^{\circ} \mathrm{C}$ and beta)
3) Select the value of the resistor $R_{\text {th }}$ as $R_{\text {th }}=T H$ at $T_{\text {threshold }}$


Figure 34 Thermal Feedback Network
The thermistor resistance, $R_{T}$, at a temperature of $T$ degrees Kelvin is given by
$R_{T}=R_{R} e^{B\left(\frac{1}{T}-\frac{1}{T_{R}}\right)}$
Where
$R_{R}$ is the thermistor resistance at the reference temperature, $T_{R}$
$T_{R}$ is the reference temperature, in Kelvin, normally $273+25=298 \mathrm{~K}\left(+25^{\circ} \mathrm{C}\right)$
$B$ is the "beta" value of the thermistor.

For example,

1) Temperature threshold $T_{\text {threshold }}=273+70=343 \mathrm{~K}\left(+70^{\circ} \mathrm{C}\right)$
2) $\mathrm{TH} 1=10 \mathrm{k} \Omega$ at $+25^{\circ} \mathrm{C}$ and $\mathrm{B}=3900 \rightarrow \mathrm{R}_{\mathrm{T}}=1.8 \mathrm{k} \Omega$ @ $+70^{\circ} \mathrm{C}$
3) $R_{t h}=R_{T}$ at $T_{\text {threshold }}=1.8 \mathrm{k} \Omega$

## Over-Temperature Shutdown

The ZXLD1370 incorporates an over-temperature shutdown circuit to protect against damage caused by excessive die temperature. A warning signal is generated on the STATUS output when die temperature exceeds $+125^{\circ} \mathrm{C}$ nominal and the output is disabled when die temperature exceeds $+150^{\circ} \mathrm{C}$ nominal. Normal operation resumes when the device cools back down to $+125^{\circ} \mathrm{C}$.

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## Application Information (cont.)

## FLAG/STATUS Outputs

The FLAG/STATUS outputs provide a warning of extreme operating or fault conditions. FLAG is an open-drain logic output, which is normally off, but switches low to indicate that a warning, or fault condition exists. STATUS is a DAC output, which is normally high ( 4.5 V ), but switches to a lower voltage to indicate the nature of the warning/fault.

Conditions monitored, the method of detection and the nominal STATUS output voltage are given in the following table:
Table 2

| Warning/Fault Condition | Severity <br> (Note 17) | Monitored Parameters | FLAG | Nominal STATUS Voltage |
| :---: | :---: | :---: | :---: | :---: |
| Normal operation |  |  | H | 4.5 |
| Supply under-voltage | 1 | $\mathrm{V}_{\text {AUX }}<5.6 \mathrm{~V}$ | L | 4.5 |
|  | 2 | $\mathrm{V}_{\text {IN }}<5.6 \mathrm{~V}$ | L | 3.6 |
| Output current out of regulation (Note 18) | 2 | $V_{\text {SHP }}$ outside normal voltage range | L | 3.6 |
| Driver stalled with switch 'on', or 'off' (Note 19) | 2 | $t_{\text {ON }}$, or $t_{\text {OFF }}>100 \mu \mathrm{~s}$ | L | 3.6 |
| Device temperature above maximum recommended operating value | 3 | Tj>+125 ${ }^{\circ} \mathrm{C}$ | L | 1.8 |
| Sense resistor current l $\mathrm{I}_{\mathrm{R}}$ above specified maximum | 4 | $V_{\text {SENSE }}>0.32 \mathrm{~V}$ | L | 0.9 |

Notes: $\quad$ 17. Severity 1 denotes lowest severity.
18. This warning will be indicated if the output power demand is higher than the available input power; the loop may not be able to maintain regulation.
19. This warning will be indicated if the gate pin stays at the same level for greater than $100 \mu \mathrm{~s}$ (e.g. the output transistor cannot pass enough current to reach the upper switching threshold).


Figure 35 Status Levels

In the event of more than one fault/warning condition occurring, the higher severity condition will take precedence. E.g. 'Excessive coil current' and 'Out of regulation' occurring together will produce an output of 0.9 V on the STATUS pin.

If $\mathrm{V}_{\text {ADJ }}>1.7 \mathrm{~V}, \mathrm{~V}_{\text {SENSE }}$ may be greater than the excess coil current threshold in normal operation and an error will be reported. Hence, STATUS and FLAG are only guaranteed for $\mathrm{V}_{\mathrm{ADJ}}<=\mathrm{V}_{\text {REF }}$.

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## Application Information (cont.)

Diagnostic signals should be ignored during the device start up for $100 \mu \mathrm{~s}$. The device start up sequence will be initiated both during the first power on of the device or after the PWM signal is kept low for more than 15 ms , initiating the standby state of the device.

In particular, during the first $100 \mu$ s the diagnostic is signaling an over-current then an out-of-regulation status. These two events are due to the charging of the inductor and are not true fault conditions.


Figure 36 Diagnostic During Start-up

## Boosting Vaux Supply Voltage in Boost and Buck-Boost Mode

When the input voltage is lower than 8 V , the gate voltage will also be lower 8 V . This means that depending on the characteristics of the external MOSFET, the gate voltage may not be enough to fully enhance the power MOSFET. This boosting technique is particularly important when the output MOSFET is operating at full current, since the boost circuit allows the gate voltage to be higher than 12V. This guarantees that the MOSFET is fully enhanced reducing both the power dissipation and the risk of thermal runaway of the MOSFET itself. An extra diode D2 and decoupling capacitor C 3 can be used, as shown below in figure 37 , to generate a boosted voltage at $\mathrm{V}_{\text {AU }}$ when the input supply voltage at $\mathrm{V}_{\text {IN }}$ is below 8 V . This enables the device to operate with full output current when $\mathrm{V}_{\mathbb{I N}}$ is at the minimum value of 6 V . In the case of a low voltage threshold MOSFET, the bootstrap circuit is generally not required.


Figure 37 Bootstrap Circuit for Boost and Buck-Boost Low Voltage Operations

The resistor R2 can be used to limit the current in the bootstrap circuit in order to reduce the impact of the circuit itself on the LED accuracy. The impact on the LED current is usually a decrease of maximum $5 \%$ compared to the nominal current value set by the sense resistor.

The Zener diode D3 is used to limit the voltage on the $\mathrm{V}_{\mathrm{Aux}}$ pin to less than 60 V .
Due to the increased number of components and the loss of current accuracy, the bootstrap circuit is recommended only when the system has to operate continuously in conditions of low input voltage (between 6 and 8 V ) and high load current. Other circumstances such as low input voltage at low load current, or transient low input voltage at high current should be evaluated keeping account of the external MOSFET power dissipation.

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## Application Information (cont.)

## Over-Voltage Protection

The ZXLD1370 is inherently protected against open-circuit load when used in Buck configuration. However care has to be taken with opencircuit load conditions in Buck-Boost or Boost configurations. This is because in these configurations there is no internal open-circuit protection mechanism for the external MOSFET. In this case an Over-Voltage-Protection (OVP) network should be provided externally to the MOSFET to avoid damage due to open circuit conditions. This is shown in figure 38 below, highlighted in the dotted blue box.


Figure 38 OVP circuit
The zener voltage is determined according to: $\mathrm{Vz}=\mathrm{V}_{\text {LEDMAX }}+10 \%$ where $\mathrm{V}_{\text {LEDMAX }}$ is maximum LED chain voltage.
If the LEDA voltage exceeds $V_{z}$ the gate of MOSFET Q2 will rise turning Q2 on. This will pull the PWM pin low and switch off Q1 until the voltage on the drain of $Q 1$ falls below $V_{z}$. If the voltage at LEDA remains above $V_{z}$ for longer than 20 ms then the $Z X L D 1370$ will enter into a shutdown state.

Care should be taken such that the maximum gate voltage of the Q2 MOSFET is not exceeded.
Take care of the max voltage drop on the Q2 MOSFET gate.

## Application Information (cont.)

## PCB Layout Considerations

PCB layout is a fundamental activity to get the most of the device in all configurations. In the following section it is possible to find some important insight to design with the ZXLD1370 both in Buck and Buck-Boost/Boost configurations.


Figure 39 Circuit Layout
Here are some considerations useful for the PCB layout:

- In order to avoid ringing due to stray inductances, the inductor L1, the anode of D1 and the drain of Q1 should be placed as close together as possible.
- The shaping capacitor C1 is fundamental for the stability of the control loop. To this end it should be placed no more than 5 mm from the SHP pin.
- Input voltage pins, VIN and VAUX, need to be decoupled. It is recommended to use two ceramic capacitors of 2.2uF, X7R, 100V (C3 and C4). In addition to these capacitors, it is suggested to add two ceramic capacitors of $1 \mathrm{uF}, \mathrm{X} 7 \mathrm{R}, 100 \mathrm{~V}$ each (C2, C8), as well as a further decoupling capacitor of 100 nF close to the VIN/VAUX pins (C9). VIN and VAUX pins can be short-circuited when the device is used in buck mode, or can be driven from a separate supply.

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## Application Information (cont.)

## Application Examples

## Example 1: 2.8A Buck LED Driver

In this application example, the ZXLD1370 is connected as a buck LED driver. The schematic and parts list are shown below. The LED driver is able to deliver 2.8 A of LED current with an input voltage range of 8 V to 24 V . In order to achieve high efficiency at high LED current, a Super Barrier Rectifier (SBR) with a low forward voltage is used as the free wheeling rectifier.

This LED driver is suitable for applications which require high LED current such as LED projector, automatic LED lighting etc.


Figure 40 Application Circuit: 2.8A Buck LED Driver
Table 3: Bill of Material

| Ref No. | Value | Part No. | Manufacturer |
| :---: | :---: | :---: | :---: |
| U1 | 60 V LED driver | ZXLD1370 | Diodes Inc |
| Q1 | 60 V MOSFET | ZXMN6A09K | Diodes Inc |
| D1 | $45 \mathrm{~V} \mathrm{10A} \mathrm{SBR}$ | SBR10U45SP5 | Diodes Inc |
| L1 | $33 \mu \mathrm{H} \mathrm{4.2A}$ | 744770933 | Wurth Electronik |
| C1 | $100 \mathrm{pF} \mathrm{50V}$ | SMD 0805/0603 | Generic |
| C2 | $1 \mathrm{uF} \mathrm{50V} \mathrm{X7R}$ | SMD1206 | Generic |
| C3 C4 C5 | $4.7 \mu \mathrm{~F} 50 \mathrm{~V} 7 \mathrm{R}$ | SMD1210 | Generic |
| R1 R2 R3 | $300 \mathrm{~m} \Omega 1 \%$ | SMD1206 | Generic |
| R4 | $400 \mathrm{~m} \Omega 1 \%$ | SMD1206 | Generic |
| R5 | $0 \Omega$ | SMD 0805/0603 | Generic |

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## Application Information (cont.)

## Typical Performance



Figure 41 Efficiency


Figure 42 Line Regulation

## Example 2: 400mA Boost LED Driver

In this application example, the ZXLD1370 is connected as a boost LED driver. The schematic and parts list are shown below. The LED driver is able to deliver 400 mA of LED current into 12 high-brightness LEDs with an input voltage range of 16 V to 32 V .

The overall high efficiency of $92 \%+$ makes it ideal for applications such as solar LED street lighting and general LED illuminations.


Figure 43 Application Circuit - $\mathbf{4 0 0 m A}$ Boost LED Driver
Table4. Bill of Material

| Ref No. | Value | Part No. | Manufacturer |
| :---: | :---: | :---: | :---: |
| U1 | 60 V LED driver | ZXLD1370 | Diodes Inc |
| Q1 | 60 V MOSFET | ZXMN6A25G | Diodes Inc |
| Q2 | 60 V MOSFET | 2N7002A | Diodes Inc |
| D1 | 100 V 3A Schottky | PDS3100-13 | Diodes Inc |
| Z1 | 47 V 410 mW Zener | BZT52C47 | Diodes Inc |
| L1 | $68 \mu \mathrm{H} 2.1 \mathrm{~A}$ | 744771168 | Wurth Electronik |
| C1 | $100 \mathrm{pF} \mathrm{50V}$ | SMD 0805/0603 | Generic |
| C3 C9 | $4.7 \mu \mathrm{~F} \mathrm{50V} \mathrm{X7R}$ | SMD1210 | Generic |
| C2 | $1 \mu \mathrm{~F} \mathrm{50V} \mathrm{X7R}$ | SMD1206 | Generic |
| R1 R2 | $560 \mathrm{~m} \Omega 1 \%$ | SMD1206 | Generic |
| R9 R10 | $33 \mathrm{k} \Omega ~ 1 \%$ | SMD 0805/0603 | Generic |
| R12 | $0 \Omega$ | SMD 0805/0603 | Generic |
| R15 | $2.7 \mathrm{k} \Omega$ | SMD 0805/0603 | Generic |

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Application Information (cont.)

400mA Boost LED Driver Typical Performance


Figure 44 Efficiency


Figure 45 Line Regulation

## Example 3: 700mA Buck-Boost LED Driver

In this application example, the ZXLD1370 is connected as a buck-boost LED driver. The schematic and parts list are shown below. The LED driver is able to deliver 700 mA of LED current into 4 high-brightness LEDs with an input voltage range of 7 V to 20 V .

Since the Buck-boost LED driver handles an input voltage range from below and above the total LED voltage, the versatile input voltage range make it ideal for automotive lighting applications.


Figure 46 Application Circuit - 700mA Buck-Boost LED Driver

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Application Information (cont.)
Table 5: Bill of Material

| Ref No. | Value | Part No. | Manufacturer |
| :---: | :---: | :---: | :---: |
| U1 | 60 V LED driver | ZXLD1370 | Diodes Inc |
| Q1 | 60 V MOSFET | ZXMN6A25G | Diodes Inc |
| Q2 | 60 V MOSFET | 2N7002A | Diodes Inc |
| D1 | 100 V 5 A Schottky | PDS5100-13 | Diodes Inc |
| Z1 | 47 V 410 mW Zener | BZT52C47 | Diodes Inc |
| L1 | $22 \mu \mathrm{H} 2.1 \mathrm{~A}$ | 744771122 | Wurth Electronik |
| C1 | $100 \mathrm{pF} \mathrm{50V}$ | SMD 0805/0603 | Generic |
| C3 C9 | $4.7 \mu \mathrm{~F} 50 \mathrm{~V}$ X7R | SMD1210 | Generic |
| C2 | $1 \mu \mathrm{~F} 50 \mathrm{~V}$ X7R | SMD1206 | Generic |
| R1 R2 R3 | $300 \mathrm{~m} \Omega 1 \%$ | SMD1206 | Generic |
| R9 | $33 \mathrm{k} \Omega 1 \%$ | SMD 0805/0603 | Generic |
| R10 | $15 \mathrm{k} \Omega 1 \%$ | SMD 0805/0603 | Generic |
| R12 | $0 \Omega$ | SMD 0805/0603 | Generic |
| R15 | $2.7 \mathrm{k} \Omega$ | SMD 0805/0603 | Generic |

700mA Buck-Boost LED Driver Typical Performance


Figure 47 Efficiency


Figure 48 Line Regulation

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## Ordering Information

| Part Number | Packaging | Status | Part Marking | Reel Quantity | Tape Width | Reel Size |
| :---: | :---: | :---: | :---: | :---: | :---: | :---: |
| ZXLD1370EST16TC | TSSOP-16EP | Active | $\begin{gathered} \text { ZXLD } \\ 1370 \\ \text { YYWW } \end{gathered}$ | 2500 | 16 mm | 13" |
| ZXLD1370QESTTC | TSSOP-16EP | Active |  | 2500 | 16 mm | 13" |

Where YY is last two digits of year and WW is two digit week number

## Package Outline Dimensions (All dimensions in mm.)

Please see AP02002 at http://www.diodes.com/datasheets/ap02002.pdf for latest version.


| TSSOP-16EP |  |  |  |  |
| :---: | :---: | :---: | :---: | :---: |
| Dim | Min | Max | Typ |  |
| A | - | 1.20 | - |  |
| A1 | 0.025 | 0.100 | - |  |
| A2 | 0.80 | 1.05 | 0.90 |  |
| b | 0.19 | 0.30 | - |  |
| C | 0.09 | 0.20 | - |  |
| D | 4.90 | 5.10 | 5.00 |  |
| E | 6.20 | 6.60 | 6.40 |  |
| E1 | 4.30 | 4.50 | 4.40 |  |
| e | 0.65 BSC |  |  |  |
| L | 0.45 | 0.75 | 0.60 |  |
| L1 | 1.0 REF |  |  |  |
| L2 | 0.65 BSC |  |  |  |
| X | - | - | 2.997 |  |
| Y | - | - | 2.997 |  |
| 日1 | $0^{\circ}$ | $8^{\circ}$ | - |  |
| All Dimensions in mm |  |  |  |  |
|  |  |  |  |  |

## Suggested Pad Layout

Please see AP02001 at http://www.diodes.com/datasheets/ap02001.pdf for the latest version.


| Dimensions | Value <br> (in mm) |
| :---: | :---: |
| $\mathbf{C}$ | 0.650 |
| $\mathbf{X}$ | 0.450 |
| $\mathbf{X 1}$ | 3.290 |
| $\mathbf{X 2}$ | 5.000 |
| $\mathbf{Y}$ | 1.450 |
| $\mathbf{Y 1}$ | 3.290 |
| $\mathbf{Y 2}$ | 4.450 |
| $\mathbf{Y 3}$ | 7.350 |

ZXLD1370

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Наши контакты:
Телефон: +7 8126271435
Электронная почта: sales@st-electron.ru
Адрес: 198099, Санкт-Петербург, Промышленная ул, дом № 19, литера H, помещение 100-Н Офис 331


[^0]:    Notes: $\quad$ 1. No purposely added lead. Fully EU Directive 2002/95/EC (RoHS) \& 2011/65/EU (RoHS 2) compliant.

[^1]:    Note: 4. Type refers to whether or not pin is an Input, Output, Input/Output or power supply pin

